

METHOD AND APPARATUS FOR CANCELLING COMMON MODE NOISE
OCCURRING IN COMMUNICATIONS CHANNELS

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DESCRIPTION

This invention relates to noise cancellation and is especially applicable to a
5 method and apparatus for cancelling common mode noise occurring in communications
channels, particularly telephone subscriber loops employing twisted-wire pairs, connected
to a receiver.

BACKGROUND ART:

10 In theory, twisting together the conductors forming a twisted-wire cable, as used
in a telephone subscriber loop, ensures that the impedance is balanced throughout its
length. In practice, however, there are imbalances. For example, moisture ingress
might cause one conductor to have greater leakage to ground, the twisting might not be
uniform, and the conductors might be untwisted where taps are made. When a signal
15 propagates along the cable, the waves on the respective conductors encounter different
complex impedances. As a result, they may propagate at different speeds and be subject
to different distortion. Upon arrival at the receiver, the two waves are no longer
symmetrical. Although this effect can usually be ignored in conventional telephone
systems, it presents problems in high speed digital subscriber loops, especially Very
20 High speed Digital Subscriber Loops (VDSL) which operate at radio frequencies.
Radio-frequency (RF) signals from commercial AM or amateur radio transmitters
frequently couple to twisted wire cables, particularly to overhead service drops, as a
common mode noise signal. Because of the above-described cable imbalance, some
portion of such an RF interference signal will usually convert to differential mode and
25 be coupled inductively across the hybrid device. In addition, the stray capacitance
between the input and output of the hybrid will couple the RF interference signal to
appear at the output of the hybrid device. This may be significant if the RF interference
signal is relatively large in amplitude.

Various systems have been proposed to cancel common mode noise in subscriber
30 loops. In T1E1.4/96-084 dated April 18, 1996, and at a VDSL workshop at IEEE
Globecom, November 18, 1996 in London, England, John Cioffi and John Bingham
proposed doing so by extracting a signal representing common mode noise and filtering
it using an adaptive analog wide band filter to provide a radio frequency noise estimate

for subtraction from the differential signal obtained from the secondary of the hybrid transformer. The coefficients of the adaptive filter were tuned during quiet periods, i.e. when no signal is being transmitted, to reduce the difference between the differential signal and the noise estimate signal substantially to zero. Unfortunately, in normal 5 operation, the adaptive analog filter cannot readily compensate for the cross-coupling of the differential signal and common mode signals due to the loop imbalance and so, during signal transmission, will cancel part of the differential information signal too. Accordingly, the resulting signal supplied to the receiver will be distorted.

Canadian patent application No. 2,237,460 filed May 13, 1998, naming one of 10 the present inventors, disclosed a noise suppression circuit in which a narrowband noise detection and control unit scanned the operating band to identify noisy frequency bands and suppressed the noise in those bands. The circuit is not entirely satisfactory because it requires the number of interfering RF signals to be few and does not cancel impulse noise. International patent application No. WO 99/63675 published December 9, 1999, 15 also naming such inventor, disclosed a wideband common mode noise canceller in which a digital common mode signal was filtered by an analysis filter bank to produce subband signals at different frequencies. Previous samples of each of the subband signals were summed and compared with a predetermined noise threshold. If the summed noise signal was greater than the threshold, the subband signal was processed by a synthesis filter to 20 form a component of a noise estimate signal for subtraction from the differential signal. While this circuit will compensate to some extent for stray capacitance of the hybrid device and the above-described loop imbalance caused by inductive coupling close to the receiver, its performance is limited since RF interference often is coupled into the loop as positions far from the receiver.

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DISCLOSURE OF INVENTION:

An object of embodiments of the present invention is to mitigate or eliminate either or both of the above-described effects of impedance imbalance and capacitive coupling.

30 According to one aspect of the present invention, a noise cancellation circuit for a communications channel comprises a differential signal path and a common mode signal path connected to respective inputs of a summing device, the differential signal path comprising input means connected to the channel for receiving a differential signal

therefrom and supplying the differential signal to a first of the inputs of the summing device, the common mode signal path comprising extraction means coupled to the channel for extracting therefrom a common mode signal, means for generating a common mode noise estimate signal and applying said estimate signal to a second of the inputs 5 of the summing device, coupling means for coupling at least part of the extracted common mode signal to an input of the generating means, the coupling means having a capacitive component equivalent to stray capacitance coupling between an input and an output, respectively, of the input means, the circuit further comprising means for compensating for phase differences between the differential signal and common mode 10 noise estimate signal before their application to the summing device, the summing device providing as an output signal of the noise cancellation circuit the difference between the differential signal and the common mode noise estimate signal.

According to a second aspect of the invention, a noise cancellation circuit for a communications channel comprises a differential signal path and a common mode signal 15 path connected to respective inputs of a digital adder, the differential signal path comprising input means connected to the channel for receiving a differential signal therefrom and analog-to-digital converter means coupled to the input means for digitizing the received differential signal and applying the digitized differential signal to a first of the inputs of the digital adder, the common mode signal path comprising extraction 20 means coupled to the channel for extracting therefrom a common mode signal, a second analog-to-digital converter means coupled to the extraction means for digitizing the extracted common mode signal and applying the digitized extracted common mode signal to a noise detector for detecting one or more noisy frequency bands of the common mode signal and passing the digitized common mode signal in those detected frequency bands 25 to an adaptive filter, the adaptive filter filtering the digitized common mode signal to produce a digital common mode noise estimate signal and applying the digital estimate signal to the second input of the digital adder, control means having inputs connected to the differential signal path and the common mode signal path and for determining correlation between signals in the differential signal path and common mode signal path 30 and adjusting coefficients of the adaptive filter in dependence thereupon so as to reduce correlation between the differential and common mode signals, the circuit further comprising means for compensating for phase differences between the differential signal and the common mode signal before their application to the digital adder, the adder

providing as an output signal of the noise cancellation circuit the difference between the differential signal and the digital common mode noise estimate signal.

In embodiments of either of the first and second aspects of the invention, the first compensating means may comprise a delay unit interposed between the input means and 5 the first summing device and having a delay period substantially equal to delay introduced in the first common mode signal path.

In embodiments of either of the first and second aspects of the invention, where the input means comprises a hybrid transformer, the capacitive coupling means comprises a second hybrid transformer similar to the first hybrid transformer, the primary winding 10 of the second hybrid transformer being short-circuited and connected to the output of the common mode signal extraction means for reception of the common mode signal and the secondary winding of the second transformer being connected to said second input of the summing device.

Embodiments of the invention may combine both aspects of the invention. Thus, 15 according to a third aspect of the invention, a noise cancellation circuit for a communications channel comprises a differential signal path and a first common mode signal path connected to respective inputs of a summing device, the differential signal path comprising input means connected to the channel for receiving a differential signal therefrom and supplying same to a first of the inputs of the summing device, the first 20 common mode signal path comprising extraction means coupled to the channel for extracting therefrom a common mode signal and coupling means connected between the common mode extraction means and a second input of the summing means for coupling an analog common mode noise estimate signal to the summing means, the coupling means having a capacitive component equivalent to stray capacitance coupling between 25 the input and the output, respectively, of the input means, and first compensating means for compensating for phase differences between the differential signal and analog common mode noise estimate signal before their application to the summing device, the output of the summing device being connected by way of an analog-to-digital converter to a first input of a digital adder means, the circuit further comprising a second common 30 mode signal path connected between the common mode signal extraction means and a second input of the digital adder, the second common mode signal path comprising a noise detector connected by way of an analog-to-digital converter to the output of the common mode extraction means, the noise detector being operable to detect one or more

noisy frequency bands of a digitized common mode signal from the analog-to-digital converter means and pass the digitized common mode signal in those detected frequency bands to an adaptive filter, the output of the adaptive filter comprising a digital common mode noise estimate signal and being applied to a second input of the digital adder means, the circuit comprising control means connected to the differential signal path and the digital common mode signal path for determining correlation between signals in the differential signal path and digital common mode signal path, respectively, and adjusting coefficients of the adaptive filter in dependence thereupon so as to reduce correlation between said signals, the circuit further comprising second compensating means for compensating for phase differences between the signal output from the first summing means and the digital common mode noise estimate signal before their application to the respective inputs of the digital adder means, the digital adder means providing as an output signal of the noise cancellation circuit the difference between the differential signal and the two common mode noise estimate signals.

15 In embodiments of either of the first and third aspects of the invention, the noise detector may comprise a bank of narrowband filters having a degree of overlap therebetween for splitting the common mode signal into a corresponding plurality of narrowband signals, selector means being controlled by the control unit to select the noisy bands, and combining means for combining signals in the selected bands to form 20 the digital common mode noise estimate signal.

The selector means may then comprise a bank of selectors each for a corresponding one of the narrowband signals, the circuit then comprising a plurality of averaging means for deriving a running average of samples of the narrowband signals, comparing such average with a corresponding threshold, and controlling the 25 corresponding selector in dependence upon such comparison, the control unit controlling the threshold levels to select the noisy bands.

The narrowband filters may comprise components of an analysis filter bank having a plurality of downsamplers each for downsampling a respective one of the narrowband signals and the combining means comprises a corresponding synthesis filter 30 bank.

The noise detector may comprise a circuit as described and claimed in copending Canadian patent application No. 2,239,675.

According to fourth, fifth and sixth aspects of the invention, there are provided noise cancellation methods corresponding to the noise cancellation circuits of the first second and third aspects.

5 BRIEF DESCRIPTION OF THE DRAWINGS:

Embodiments of the invention will now be described by way of example only and with reference to the accompanying drawings in which:-

Figure 1 illustrates a first embodiment of the invention in the form of a noise canceller with capacitive coupling;

- 10 Figure 2 illustrates a capacitive coupling device of the embodiment of Figure 1;
- Figure 3 illustrates a second embodiment of the invention in the form of a noise canceller having a noise detector and an adaptive filter;
- Figure 4 illustrates a suitable noise detector for the embodiment of Figure 3;
- Figure 5 illustrates functions of a control unit of the embodiment of Figure 3; and
- 15 Figure 6 illustrates a third embodiment of the invention which combines the embodiments of Figures 1 and 3.

BEST MODES FOR CARRYING OUT THE INVENTION:

In the drawings, identical or corresponding items in the different figures have the 20 same reference numeral, in some cases with a suffix or prime to indicate a modification.

Figure 1 illustrates, schematically, a noise suppression circuit according to a first embodiment of the invention connected to a communications channel. More specifically, the communications channel comprises a twisted-wire pair subscriber loop having the TIP and RING wires 10 and 12 connected to input means, specifically respective ends of the 25 primary winding 14P of a hybrid transformer 14 and also to respective inputs of a summer 16 which extracts a common mode signal. The secondary winding 14S of the hybrid transformer 14 has one end grounded and the other end connected by way of a variable-gain amplifier 26 and an analog delay line 28 to one input of a summer 24, the output of which is coupled to the usual receiver (not shown). The hybrid transformer 30 14 converts the signal received from the subscriber loop 10 to a differential signal which includes a component corresponding to common mode noise in the received signal. The summer 24 subtracts from the differential signal a common mode noise estimate signal derived from the output of the summer 16, which is supplied by way of a second

variable gain amplifier 18, a capacitive coupling device 20 and an inverting amplifier 22 to a second input of the summer 24. During manufacture, the delay provided by the analog delay unit 28 is adjusted to compensate for delay introduced in the common mode path, specifically by the amplifiers 18 and 22 and the capacitive coupling device 20, so that the common mode estimate signal is synchronized with the different signal at the summer 24. Likewise, the gains in the differential signal path and common mode signal path are adjusted by adjusting the respective gains of the amplifiers 18 and 26 so that the amplitude of the common mode noise estimate signal will correspond to that of the common mode noise component of the differential signal. The gain of the amplifier 18 is proportional to the gain of amplifier 26.

As illustrated in Figure 2, the capacitive coupling device 20 conveniently comprises a second hybrid transformer 30 substantially identical to the hybrid transformer 14. The primary winding 30P of second transformer 30 is short-circuited and connected to the output of amplifier 18, while its secondary winding 30S has one end grounded and the other end connected to the amplifier 22. Because the primary winding 30P is short-circuited, the common mode signal will be coupled to the amplifier 22 by way of the stray capacitive coupling of the second transformer 30, which should be substantially the same as the stray capacitive coupling of the first transformer 14. Consequently, the noise estimate signal subtracted from the differential signal should correspond to that coupled across the stray capacitance of the first transformer 14.

Where the subscriber loop is well-balanced, and relatively short, say a few hundred meters long, the noise cancellation circuit of Figure 1 might be sufficient. In many cases, however, the subscriber loop is not well-balanced and it is necessary to compensate for such imbalance. The noise cancellation circuit illustrated in Figure 3 compensates for loop imbalance.

Figure 3 illustrates a noise cancellation circuit according to a second embodiment of the invention which compensates for loop imbalance. The noise cancellation circuit comprises a differential signal path comprising a hybrid transformer 14 having its primary winding 14P connected to the TIP 10 and RING 12 of a twisted-wire pair subscriber loop. One end of its secondary winding 14S is grounded and the other end is connected to an input of a variable gain amplifier 26. The output of amplifier 26 is connected by way of an analog-to-digital converter 42 and digital delay unit 44 to a first input of a digital adder 46. The adder 46 subtracts from the delayed differential signal

a common mode noise estimate signal which is derived via a common mode signal path comprising the summer 16, a variable gain amplifier 18, a second analog-to-digital converter 48, a digital noise detector (DND) 50 and an adaptive filter 52. The digitized common mode signal is applied to the digital noise detector which detects the frequency 5 bands in which there is significant noise and passes to the adaptive filter 52 only the signal in those bands. The adaptive filter 52 is controlled by a control unit 54, specifically a microcontroller, which has inputs connected to the differential path at the output of the A/D converter 42, to the common mode signal path at the output of the A/D converter 48, to the output of the digital noise detector 50 and to the output of the 10 adder 46, which constitutes the output of the noise cancellation circuit. As illustrated by functional blocks 5.1 and 5.2 of Figure 5, which illustrates pertinent functions of the control unit/microcontroller 54, the latter also controls the gains of amplifiers 26 and 18 to ensure that the signals applied to the A/D converters 42 and 48, respectively, are within their proper operating ranges.

15 The digital delay 44 is adjusted during manufacture to compensate for delay introduced by summing device 16, amplifier 18, A/D converter 48 and digital noise detector 50. Although the adaptive filter 52 is in the common mode signal path, it need not be taken into account because its normal operation entails compensating for delays.

It should be noted that the noise canceller of Figure 3 does not need quiet periods 20 but will adapt the coefficients of adaptive filter 52 during normal operation. Thus, in operation, the common mode signal is digitized and applied to the digital noise detector 50 which will detect significant noise signals; these noise signals are, of course, most likely to have been inductively coupled into the twisted-wire pair. Only the portion of the common mode signal in the noisy frequency bands will be passed to the adaptive 25 filter 52 as the noise estimate signal. The control unit 54 monitors the cross-correlation between the output of the digital noise detector 50 and the output of the output adder 46 and tunes the coefficients of the adaptive filter 52 so as to reduce the correlation - substantially to zero. A significant advantage of this embodiment is that it does not require a quiet period to tune the adaptive filter.

30 A preferred adaptive filter 52 processes the common-mode noise signal from DND 50 such that it is as close as possible to the common mode noise component of the differential signal at the input to adder 46 by iteratively adjusting the coefficients (tap weights). The design of such an adaptive filter is known to persons skilled in this art

and so is not further discussed here; a good description can be found in an article by Bernard Widrow *et al.* entitled "Adaptive Noise Cancellation: Principles and Applications", *Proceedings of the IEEE*, Vol. 63, No. 12, December 1975, pp. 1692-1716.

5 A suitable digital noise detector (DND) 50 is disclosed in copending Canadian patent application No. 2,239,675 and will now be described with reference to Figure 4. In the digital noise detector 50, the digital common mode signal from A/D converter 48 (Figure 3) is supplied to an analysis filter bank 60 which comprises a lowpass filter 61₁, a plurality of bandpass filters 61₂ to 61_{M-1} each having a different centre frequency, and 10 a highpass filter 61_M. The narrowband signals from the filters 61₁ to 61_M are supplied to respective ones of a corresponding plurality of downsamplers 62₁ to 62_M, each of which downsamples by a factor M. In this preferred embodiment, the downsampling rate M is equal to the number of subbands, i.e., the analysis filter bank 60 is uniformly, maximally decimated.

15 The plurality of subband signals S₁ to S_M are applied to a corresponding plurality of noise detection circuits 63₁ to 63_M, respectively, the outputs of which comprise respective subband noise estimate signals E₁ to E_M. The subband noise estimate signals E₁ to E_M are supplied to respective inputs of a synthesis filter bank 64. The analysis filter bank 60 and the synthesis filter bank 64 are complementary and designed to 20 provide "pseudo perfect reconstruction" as described earlier. Thus, synthesis filter bank 64 comprises a plurality of upsamplers 65₁ to 65_M which receive and upsample the digital subband noise estimate signals E₁ to E_M, respectively, by the factor M (the same as the downsampling rate in the analysis filter 60). The outputs of the upsamplers 65₁ to 65_M are supplied to a corresponding plurality of bandpass filters 66₁ to 66_M, respectively. 25 The outputs of the filters 66₁ to 66_M are summed by summing device 67 for output to the adaptive filter 52 (Figure 3). It should be noted that the filters 66₁ to 66_M in the synthesis filter bank 64 are not identical to the corresponding filters 61₁ to 61_M in the analysis filter bank 60. The relationship between the analysis filter bank 60 and the synthesis filter bank 64, and especially the coefficients of their filters, is known to those 30 skilled in this art and so will not be described in detail here. For details, the reader is directed to chapter 7 entitled "Multirate Signal Processing" of the text book "Advanced Digital Signal Processing: Theory and Applications", by G. Zelniker and F. Taylor,

publ. Marcel Dekker, Inc., and to the technical literature, including the articles by Akansu *et al* and by Crosier *et al* (*supra*).

The noise detection circuits 63₁ to 63_M have identical structures so only one circuit 63_M, is shown in detail in Figure 4, for simplicity.

5 The components of the noise detection circuit 63_M are controlled by a common clock which, for convenience of illustration, is not shown. Within the noise detection circuit 63_M, each sample value of the subband signal S_M is applied to one input of a selector 68_M, which may be a multiplexer, and to an absolute value device 69_M which strips off the sign and supplies the sample value to an input of a delay bank 70_M. The 10 outputs of the delay bank 70_M are supplied in parallel to a summing device 71_M, which sums them and supplies the sum to a comparator 72_M. The selector 68_M is controlled by the output of the comparator 72_M to select either the instant sample of the subband signal or a zero value and supply it to the corresponding input of the synthesis filter bank 64. The subband signal S_M is clocked through the delay bank 70_M continuously. The values 15 in the delay bank 70_M in any clock cycle are summed by the summing device 71_M and the summation value compared with a threshold value T_M. If the summation value is greater than the threshold value T_M, the output of comparator 72_M is a "1" causing selector 68_M to select the instant sample value of the subband signal S_M, and supply it as the digital noise estimate signal E_M for channel M to the corresponding input of 20 synthesis filter bank 64. If the summation value is less than the threshold T, the comparator 72_M supplies a zero to selector 68_M causing it to provide a zero value as the digital noise estimate signal E_M. Thus, when the subband signal S_M contains a certain common mode noise component, the instant sample value of subband signal S_M is supplied as the digital noise estimate signal E_M. Otherwise, no value is supplied.

25 The other noise detection and phase inversion circuits 63₁ to 63_{M-1} produce corresponding digital noise estimate signals E₁ to E_{M-1} in a similar manner.

The phase inversion units 63₁ to 63_M use threshold values T₁ to T_M, respectively, which are adjusted individually by the control unit 54 (Figure 3).

Generally, each threshold value will be selected according to the nature of the 30 noise in the corresponding subband frequency band. In general, impulse noise will tend to be rather large in amplitude compared to radio frequency interference but of shorter duration. Consequently, each threshold value T₁ to T_M may be selected so that the threshold value will be exceeded if a small number of segments of the corresponding one

of the delay banks 70₁ to 70_M contain relatively high values; or all of the segments of the delay bank contain somewhat lower values, as would occur with a radio frequency interference signal. Hence, the length of the delay banks 70₁ to 70_M, any scaling factors of the signal supplied to the analysis filter bank, and the threshold would be arranged or 5 could be adjusted to suit particular conditions prevailing in the vicinity of the installation.

It should be appreciated that, although the specific embodiment uses a uniformly, maximally decimated analysis filter bank, other structures are feasible. For example, the analysis filter bank could provide a plurality of subband signals concentrated at the higher frequencies where radio frequency or impulse noise might be a greater problem 10 due to the relatively lower energy of the transmitted signal.

For further information about the digital noise detector, and examples of the various possible configurations for the digital noise detector 50, the reader is directed to the afore-mentioned Canadian patent application No. 2,239,675.

It should be noted that the digital noise detector 50 provides a history of the 15 common mode signal over several samples. It has been proposed, however, in the context of high speed digital subscriber loops, to detect noise in the received signal by comparing the power spectral density of each block of the received signal with a predefined desired spectral mask for the received (information) signal. If that is done, the digital noise detector 50 illustrated in Figure 4 could be modified by omitting, in the 20 noise detectors 63₁ to 63_M, the absolute value devices 69₁ to 69_M, the delay banks 70₁ to 70_M, the summing devices 71₁ to 71_M and the comparators 72₁ to 72_M. The subband signals S₁ to S_M then are applied directly to the selectors 68₁ to 68_M, respectively. The microcontroller 54 will then supply control signals T₁ to T_M directly to the selectors 68₁ to 25 68_M, respectively. It should be appreciated that the signals T₁ to T_M will not be threshold signals but rather 1 bit control signals to toggle the selectors.

It is also envisaged that the downsamplers 62₁ to 62_M in the analysis filter bank 60 and the upsamplers 65₁ to 65_M in the synthesis filter bank 64 might be omitted. As mentioned earlier, the passbands of the filters 61₁ to 61_M and filters 66₁ to 66_M must have the required degree of overlap.

30 When such a modified digital noise detector is used, the control unit 54 will compare the spectral power density of the received signal with a prescribed power spectral density mask or template to detect those bands in which significant noise occurs. Referring now to Figure 5, in step 5.3 the microcontroller 54 partitions the received

differential signal from A/D converter 42 into blocks each of length N samples, for example 240 samples. In step 5.4, the microcontroller uses Fast Fourier Transform (FFT) to obtain the power spectral density of each block and, in step 5.5, compares the resulting spectral envelope with a spectral mask previously stored in the 5 microcontroller's memory (not shown). It is expected that the parameters of the spectral mask will be set by national or international standards on the basis of experiments conducted with various kinds of communications channels or loops.

In step 5.6, the microcontroller lists the frequency bands in which the power spectral density of the block exceeds the envelope of the spectral mask and stores the 10 information. In step 5.7, determines for each band whether or not the power spectral density exceeded the envelope in a predetermined number X of a predetermined previous number Y of the blocks. If it did, the microcontroller adjusts the corresponding one of the signals T_1 to T_M to select that band so that the digital noise detector 50 will sum the common mode noise signal in each of those bands to produce the common mode noise 15 signal for application to the adaptive filter 52.

It is important that the digital noise detector not introduce any extra noise that might be correlated in some way with the information signal. Similarly, the DND cannot afford to make frequent changes to its output, as such activity could prevent the adaptive filter from converging properly. This can be assured by providing a suitable 20 length of delay banks 70_1 to 70_M , where the DND of Figure 4 is used, and/or by ensuring that the number of blocks X in step 5.7 is sufficient.

Figure 5 also illustrates the cross-correlation function of the microcontroller 54, which will be performed whether the digital noise detector 50 is as shown in Figure 4 or modified as described hereinbefore. Thus, step 5.8 determines cross-correlation 25 between the common mode signal from digital noise detector 50 and the system output from adder 46 and step 5.9 adjusts the coefficients of the adaptive filter 52 to reduce any such correlation, ideally to zero.

Figure 6 illustrates a third embodiment of the invention which employs both the stray capacitive coupling compensation of the embodiment of Figure 1 and the adaptive 30 filter compensation approach of the embodiment of Figure 3. As in both of the first and second embodiments, the TIP conductor 10 and RING conductor 12 are connected to the primary winding 14P of the hybrid transformer 14, the secondary winding 14S having one end grounded and the other end connected to the differential signal path, i.e. to

variable gain amplifier 26. It should be noted, however, that the differential path of the circuit illustrated in Figure 6 comprises an analog portion formed by analog delay device 28 and analog summer 24 and a digital portion formed by an A/D converter 42, a digital delay 44 and a digital adder 46, the output of the latter being the output of the noise cancellation circuit and applied to the usual receiver.

The circuit has both an analog common mode path similar to that shown in Figure 1 and a digital common mode path similar to that shown in Figure 3. The summer 16 is shared by both paths. As in the embodiment of Figure 1, the analog common mode path comprises a variable gain amplifier 18, which has a gain G2 proportional to the gain G1 of variable amplifier 26, a capacitive coupling device 20 and an inverting amplifier 22, the output of which is connected to the second input of summer 24, as before. In this circuit, however, the output of analog summer 24 is digitized by A/D converter 42 and supplied to digital delay 44 which supplies the delayed differential signal to a first input of digital adder 46. The output of summer 16 is also supplied to an input of a third variable gain amplifier 56 which has a gain G3. The output of the amplifier 56 is digitized by second A/D converter 48 and supplied to the digital noise detector 50 and the control unit 54' which detects the noisy bands and passes only the signals in those bands to the adaptive filter 52. As in the embodiment of Figure 3, the control unit/microcontroller 54 receives inputs also from the respective outputs of A/D converter 42, digital adder 46, and digital noise detector 50.

The control unit 54' will differ from the control unit 54 of Figure 3 because it will control the gains G1, G2 and G3 of the three amplifiers 26, 18 and 56, respectively. Its control of the adaptive filter 52 will be as described with reference to Figures 3 and 4 or Figures 3 and 5, i.e. using threshold control signals or selector control signals, depending upon the nature of digital noise detector 50. As before, if the DND 50 shown in Figure 6 is that shown in Figure 4, which performs historical analysis of the received signal, the microcontroller 54 need not conduct spectral analysis. If the DND 50 does not perform historical analysis, the microcontroller 54 will perform the spectral analysis and comparison described with respect to Figure 5.

The invention embraces various other modification and improvements to the above-described embodiments. Thus, control unit 54 could extract differential and common mode signals from other points in the differential signal path and common mode signal path, respectively.

It should be appreciated that the various aspects of the invention are not necessarily limited to noise cancellation in twisted pair subscriber loops but could be applied to other communications channels, in which case the input means might not be a hybrid transformer. For example, the embodiment of Figure 3 could be used with 5 communications channels which employ coaxial cables, comprising a coaxial shield and one or more inner conductors. In such a case, the hybrid transformer shown in Figure 3 would be omitted and the coaxial shield connected directly to the input of amplifier 18. Where a single inner conductor was used, it would be connected directly to the input of amplifier 26. If two or more inner conductors were used, they would be interfaced to 10 the noise detection circuit by way of a suitable matching transformer.

It should be appreciated that, although the above-described embodiment of the invention use analog components to provide the compensation for the capacitive coupling, the compensation could be implemented digitally, perhaps using a digital signal processor.

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INDUSTRIAL APPLICABILITY

Embodiments of the invention advantageously provide noise cancellation for communications channels, such as telephone subscriber loops, which compensates for the effects of stray capacitive coupling in the hybrid and/or impedance imbalance effects in the communications channel yet do not require a quiet period for training purposes.